

Learning a Common Dictionary for CSI Feedback in FDD Massive MU-MIMO-OFDM Systems

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Pavan Kumar Gadamsetty and K.V.S. Hari would like to acknowledge the support of the British Telecom India Research Centre (BTIRC), Indian Institute of Science, Bangalore. L. Hanzo would like to acknowledge the financial support of the Engineering and Physical Sciences Research Council projects EP/W016605/1, EP/X01228X/1 and EP/X01228X/1 as well as of the European Research Council's Advanced Fellow Grant QuantCom (Grant No. 789028).

ABSTRACT In a transmit preprocessing aided frequency division duplex (FDD) massive multi-user (MU) multiple-input multiple-output (MIMO) scheme assisted orthogonal frequency-division multiplexing (OFDM) system, it is required to feed back the frequency domain channel transfer function (FDCHTF) of each subcarrier at the user equipment (UE) to the base station (BS). The amount of channel state information (CSI) to be fed back to the BS increases linearly with the number of antennas and subcarriers, which may become excessive. Hence we propose a novel CSI feedback compression algorithm based on compressive sensing (CS) by designing a common dictionary (CD) to reduce the CSI feedback of existing algorithms. Most of the prior work on CSI feedback compression considered single-UE systems. Explicitly, we propose a common dictionary learning (CDL) framework for practical frequency-selective channels and design a CD suitable for both single-UE and multi-UE systems. A set of two methods is proposed. Specifically, the first one is the CDL-K singular value decomposition (KSVD) method, which uses the K-SVD algorithm. The second one is the CDL-orthogonal Procrustes (OP) method, which relies on solving the orthogonal Procrustes problem. The CD conceived for exploiting the spatial correlation of channels across all the subcarriers and UEs compresses the CSI at each UE, and upon reception reconstructs it at the BS. Our simulation results show that the proposed dictionary's estimated channel vectors have lower normalized mean-squared error (NMSE) than the traditional fixed Discrete Fourier Transform (DFT) based dictionary. The CSI feedback is reduced by 50%, and the memory reduction at both the UE and BS starts from 50% and increases with the number of subcarriers.

INDEX TERMS Wideband, frequency domain channel transfer function (FDCHTF), channel state information (CSI), compressive sensing (CS), massive MIMO, common dictionary learning (CDL), common dictionary (CD), orthogonal Procrustes (OP) problem, K-SVD algorithm.

I. INTRODUCTION

Massive multiple-input multiple-output (MIMO) systems constitute a promising enabling technique for 5G/6G cellular networks as a benefit of their substantial spatial multiplexing gain [1] in both time division duplex (TDD) and frequency division duplex (FDD) scenarios. At the base station (BS), combining the massive MIMO technology with orthogonal frequency-division multiplexing (OFDM) is capable of

transmitting multiple data symbols to multiple UEs on the same time-frequency resource block, resulting in increased system throughput [2]. In a multi-user (MU) massive MIMO-OFDM system, the knowledge of CSI¹ is needed at the BS to implement transmit precoding (TPC) for suppressing the co-channel interference (CCI) [3]. In FDD systems, due to the absence of channel reciprocity [4], the user equipment

¹We use the terms CSI and FDCHTF interchangeably

(UE) has to feed back the downlink (DL) frequency domain channel transfer function (FDCHTF) of each subcarrier to the BS. Feeding back the accurate CSI becomes more challenging with the increased number of antennas, subcarriers, and UEs [5].

The compression of high-dimensional CSI is essential for reducing the CSI feedback. The wireless channels can be represented in a sparse form in the spatial-frequency domain using ‘sparsifying’ bases termed as a dictionary [6]. In the compressive sensing (CS)-based feedback schemes [7], the original CSI is mapped to a sparse domain using a dictionary. The traditional choice of the dictionary is a fixed Discrete Fourier Transform (DFT) matrix. Then a random Gaussian measurement matrix is introduced to compress the sparse vector for feeding it back to the BS at a reduced rate. The sparse signal is then reconstructed at the BS using CS-based algorithms, such as the orthogonal matching pursuit (OMP) [8], basis pursuit (BP) [9] or covariance-assisted matching pursuit (CAMP) [10] procedures. The original CSI is then reconstructed by mapping the regenerated sparse signal back to the same dictionary used at the UE side.

The authors of [11] proposed a rotated version of the DFT basis to provide improved sparsity that results in reduced CSI mean-squared error (MSE) for a narrowband multi-user system with each UE having a single receive antenna. However, the proposed rotated basis does not exploit the antennas’ spatial correlation. The massive MIMO-OFDM channel between a multi-antenna UE and the BS can be represented by a matrix [12]. In such systems, the UE has to feed back the FDCHTF of each subcarrier, which results in huge feedback overhead. The FDCHTF feedback algorithm of a massive MIMO-OFDM single-UE system based on multidimensional compressive sensing theory using Tucker’s tensor decomposition model is developed in [13]. Briefly, Tucker’s tensor decomposition exploits the structure hidden in all the dimensions of the channel matrix and compresses it simultaneously in each dimension. The proposed scheme has a significant feedback reduction and hence improves the spectral efficiency. However, both the basis and measurement matrices should be learned. The authors of [14] introduced a recursive least squares dictionary learning algorithm (RLS-DLA) for CSI feedback. The proposed scheme achieves a substantial reduction in feedback requirements, however it requires the computation of large matrix inverses during the dictionary learning process.

Another line of work focused on designing non-dictionary-based methods for FDCHTF feedback [19]. In [20], an antenna grouping-based method was proposed for reducing the feedback overhead by grouping multiple correlated antenna elements into a single representative value. By considering a ray-based channel model, the authors of [21] and [22] designed an angle-of-departure (AoD) based adaptive subspace codebook for feedback compression. In [16] and [23] the authors exploited the low-rank characteristics of a large channel matrix for recovering the CSI at the BS.

Recent solutions include Deep Learning (DL) techniques conceived for CSI compression and recovery using so-called the Bi-LSTM [24], CsiNet-LSTM [25], DNNNet [26], CS-ReNet [27], and DCRNet [28] frameworks². Additionally, the application of Deep unfolding techniques has also shown promising results, as demonstrated in [29], [30]. These techniques have better reconstruction performance than the conventional CS algorithms of [31], albeit at significantly increased computational complexity.

Massive MIMO-OFDM channels tend to be individually sparse and simultaneously share a common support set that typically exhibit joint sparsity in the time domain (TD) [32], which results in correlation among subcarriers in the frequency domain (FD). Since the DFT dictionary does not exploit spatial correlation across antenna arrays, we design a dictionary for massive MIMO-OFDM systems that can exploit the spatial correlation, hence achieving improved CSI reconstruction performance. The dictionary is generally learned from a training data set by relying on learning-based approaches [17], [18], [33]–[35]. The dictionaries learned have the potential to offer improved normalized mean squared error (NMSE) performance compared to fixed dictionaries, like the DFT-based one. In [15] a CS-based method was proposed, which exploited the spatial correlation among the antennas in a narrowband single-UE system using the K-SVD [36] algorithm. The method relies on learning the K-SVD dictionary from the training data set and on feeding back the K-SVD dictionary learned at the UE to the BS. Using this K-SVD dictionary, the CSI is compressed at the UE and reconstructed at the BS. The motivation for this K-SVD based dictionary is not only to reduce the CSI feedback, but also to reduce the NMSE of CSI reconstruction.

As the channel-induced dispersion is increased, the number of OFDM subcarriers also has to be increased to avoid an excessive performance degradation. Hence upon using the K-SVD algorithm of [15], the number of subcarrier K-SVD based dictionaries increases as the number of subcarriers increases. Handling ubiquitous subcarrier K-SVD based dictionaries is cumbersome in terms of memory management and feedback load. To circumvent this problem, we propose a novel common dictionary learning (CDL) technique, which can replace the requirement of individual subcarrier K-SVD dictionaries, leading to the concept of a common dictionary (CD). The CD effectively captures the channel characteristics of all the subcarriers and UEs, making it the optimal sparsifying dictionary for representing the channel’s sparsity in massive MIMO systems. Given the CD learned, compressive channel estimation techniques can be constructed for acquiring the CSI. A set of two methods having different pros and cons are proposed for CDL, namely the CDL-KSVD method and the CDL-orthogonal Procrustes (OP) [37] based method. These methods are detailed in Section III of the paper. Again, our primary motivation is to reduce the CSI feedback overhead on the uplink as well

²For the expansion of these acronyms please refer to the relevant papers

TABLE 1: COMPARING OUR CONTRIBUTION TO THE EXISTING LITERATURE

| | [11] | [14] | [15] | [16] | [17] | [18] | Our |
|-------------------------------|------|------|------|------|------|------|-----|
| Massive MIMO architecture | ✓ | ✓ | ✓ | ✓ | ✓ | ✓ | ✓ |
| Spatially correlated channels | ✓ | ✓ | ✓ | ✓ | | | ✓ |
| Sparsity | ✓ | ✓ | ✓ | | ✓ | ✓ | ✓ |
| Dictionary learning | | ✓ | ✓ | | ✓ | ✓ | ✓ |
| Feedback savings | ✓ | ✓ | ✓ | ✓ | ✓ | ✓ | ✓ |
| Memory savings at UE | | | | | ✓ | | ✓ |
| Multi-user MIMO OFDM | | | | | ✓ | | ✓ |
| UE mobility | | | | | | | ✓ |

TABLE 2: LIST OF ACRONYMS

| Acronyms | Meaning |
|----------|---|
| AOD | Angle-of-Departure |
| BER | Bit Error Rate |
| BS | Base Station |
| CD | Common Dictionary |
| CDL | Common Dictionary Learning |
| CFR | Channel Frequency Response |
| CIR | Channel Impulse Response |
| CS | Compressive Sensing |
| CSI | Channel State Information |
| DFT | Discrete Fourier Transform |
| DL | Deep Learning |
| FD | Frequency Domain |
| FDD | Frequency Division Duplex |
| FDCHTF | Frequency Domain Channel Transfer Function |
| GR-SVD | Golub-Reinsch SVD |
| K-SVD | K Singular Value Decomposition |
| MIMO | Multiple-Input Multiple-Output |
| MP | Matching Pursuit |
| MSE | Mean Squared Error |
| MU | Multi User |
| NMSE | Normalized Mean Squared Error |
| OF | Objective Function |
| OFDM | Orthogonal Frequency Division Multiplexing |
| OMP | Orthogonal Matching Pursuit |
| OP | Orthogonal Procrustes |
| QuaDRiGa | Quasi Deterministic Radio Channel Generator |
| RA | Receive Antenna |
| SU | Single User |
| TA | Transmit Antenna |
| TD | Time Domain |
| TDD | Time Division Duplex |
| TPC | Transmit Precoding |
| UE | User Equipment |
| VQC | Vector Quantization Codebook |

as the memory requirement at both the UE and the BS in FDD massive MU-MIMO-OFDM systems.

Main contributions of this article:

- 1) We proposed a novel CDL framework for learning a CD, mainly using the CDL-KSVD and the CDL-OP methods. In the CDL framework proposed for a multi-UE system, the CD conceived exploits the spatial correlation of the FD channels across all the subcarriers and the UEs. We demonstrate that this implementation improves the NMSE performance when compared to the existing methods.
- 2) In the CDL framework proposed for a single-UE system, the learning of CD is implemented at the UE. The UE sends only the CD to the BS in the uplink instead of all the subcarrier K-SVD dictionaries. This implementation reduces the dictionary feedback to the BS by a factor of N_c and also reduces the memory requirement by having a single CD at the UE and the BS.
- 3) We evaluate the proposed CD in the context of various system configurations and channel conditions in the face of UE mobility. The numerical results show a significant reduction in the NMSE of channel estimation and highlight the bit error rate (BER) performance of the channel estimates when using our learned dictionary. This corroborates the effectiveness of the CDL framework proposed over existing methods in wideband massive MIMO systems.

The remainder of this paper is organized as follows. Section II presents the system model, CS procedure, and the motivation. In Section III, the proposed methods are discussed. Then the application of the proposed methods in wideband systems is discussed in Section IV. Our simulation results are provided in Section V to show the NMSE performance of the proposed method compared to state-of-the-art methods. Finally, in Section VI, our conclusions are given.

Notations: We use lower (upper) bold letters to denote column vectors (matrices) and super-scripts $(\cdot)^{-1}, (\cdot)^*, (\cdot)^H$ to represent the inverse, complex conjugate and Hermitian operators respectively, $\|\cdot\|_F$ denotes the Frobenius norm of a matrix; \otimes denotes the Kronecker product, $\text{tr}(\cdot)$ is the trace

TABLE 3: LIST OF NOTATIONS

| | |
|------------------------------------|---|
| $N_t(N_r)$ | Number of TAs (RAs) |
| L | Number of channel taps in TD |
| i | Index of the channel tap |
| N_c | Number of subcarriers in FD |
| l | Index of the subcarrier |
| K | Number of UEs |
| k | Index of the UE |
| V | Velocity of the UE |
| S | Sparsity index |
| n | Frame index |
| Ψ | Dictionary |
| Φ | Measurement (Sensing) matrix |
| Θ | Product of a dictionary and Φ |
| N_g | Number of rows in Φ |
| g | Compression factor |
| M' | Total number of training channel vectors |
| N | Number of training channel vectors considered across each subcarrier |
| UE_k | k -th user equipment |
| \mathbf{R}_{BS} | Spatial correlation matrix at the BS |
| $\mathbf{R}_{UE,k}$ | Spatial correlation matrix at the k -th UE |
| $\mathbf{H}_{n,k}$ | TD channel matrix across the n -th tap of the k -th UE |
| $\check{\mathbf{H}}_{n,k}$ | TD i.i.d channel matrix |
| \mathbf{H} | Concatenated channel matrix of K UEs |
| \mathbf{H}_k | Channel matrix of the k -th UE |
| $\hat{\mathbf{H}}_k$ | Reconstructed channel matrix of the k -th UE at the BS |
| \mathbf{H}' | Matrix of training channel vectors at the UE |
| $\tilde{\mathbf{H}}'$ | Sparse channel matrix representation of \mathbf{H}' |
| $\hat{\mathbf{H}}'$ | Matrix of reconstructed training channel vectors at the BS |
| $\hat{\tilde{\mathbf{H}}}'$ | Sparse channel matrix representation of $\hat{\mathbf{H}}'$ |
| $\mathbf{H}_{l,n,k}$ | Channel matrix or FDCHTF across the l -th subcarrier of the k -th UE in n -th frame |
| $\hat{\mathbf{H}}_{l,n,k}$ | Reconstructed channel matrix across the l -th subcarrier of the k -th UE in n -th frame |
| $\mathbf{h}_{l,n,k}$ | Channel vector transformation of $\mathbf{H}_{l,n,k}$ |
| $\tilde{\mathbf{h}}_{l,n,k}$ | Sparse channel vector representation of $\mathbf{h}_{l,n,k}$ |
| $\hat{\mathbf{h}}_{l,n,k}$ | Channel vector transformation of $\hat{\mathbf{H}}_{l,n,k}$ |
| $\tilde{\hat{\mathbf{h}}}_{l,n,k}$ | Sparse channel vector representation of $\hat{\mathbf{H}}_{l,n,k}$ |
| $\mathbf{h}_{c,l,n}^k$ | Compressed channel vector across the l -th subcarrier of the k -th UE in n -th frame |
| Ψ_{DFT} | DFT dictionary |
| $\Psi_{ksvd,l}^k$ | K-SVD dictionary across the l -th subcarrier of the k -th UE |
| Ψ_c | Common dictionary |
| Δ_{saved} | Total memory storage reduction |
| Υ | Dictionary feedback reduction factor |
| \mathcal{T}_{ksvd} | Feedback required for sending N_c subcarrier dictionaries |
| \mathcal{T}_{com} | Feedback required for sending Ψ_c |
| \mathcal{T}_{saved} | Total dictionary feedback reduction |

TABLE 4: References for CSI compression techniques

| | Single-UE | Multi-UE |
|------------|---|---|
| Narrowband | CS basis [14], [31] | Rotated DFT [11] K-SVD dictionary [15] Bi-LSTM [24] |
| Wideband | Multidimensional CSI [17] CsiNet [38] CsiNet-LSTM [25] DNNNet [26] | CS-ReNet [27] |

of the matrix, $\text{vec}(\cdot)$ operation returns a column vector by stacking all the columns of a matrix.

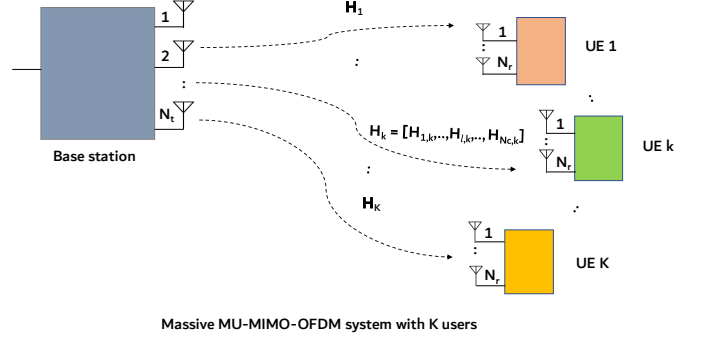


FIGURE 1: Overview of the considered massive MU-MIMO-OFDM system. Right: K UEs with N_r RAs each for $k = 1$ to K ; Left: massive MIMO base station with N_t TAs. \mathbf{H}_k represents the complete FDCHTF of the k -th UE and $\mathbf{H}_{l,k}$ represents the FDCHTF across the l -th subcarrier of the k -th UE.

II. System Model

In this section, we first introduce the massive MU-MIMO-OFDM channel and the associated spatial correlation matrices at the BS and UEs. Furthermore, we conceive the CS-based channel reconstruction procedure of massive MIMO channels. Next, we highlight the dictionary learning algorithms available in the literature. Then, in the final subsection we describe the motivation of the proposed CDL framework.

A. The Massive MU-MIMO-OFDM Channel

We consider a massive MU-MIMO-OFDM system using a uniform linear array (ULA) of N_t TAs at the BS, N_r RAs at all the K UEs and N_c subcarriers. For the k -th UE ($k = 1$ to K), consider a frequency-selective channel having L taps in the TD. Let $\mathbf{H}_{l,k}$ represent the FDCHTF of the l -th subcarrier of the k -th UE given by

$$\mathbf{H}_{l,k} = \sum_{i=0}^{L-1} \bar{\mathbf{H}}_{i,k} e^{-\frac{j2\pi il}{N_c}}, \quad (1)$$

where $\bar{\mathbf{H}}_{i,k} \in \mathbb{C}^{N_r \times N_t}$ is the i -th tap TD channel matrix. The tap coefficient $\bar{\mathbf{H}}_{i,k}(p, q)$ represents the channel impulse

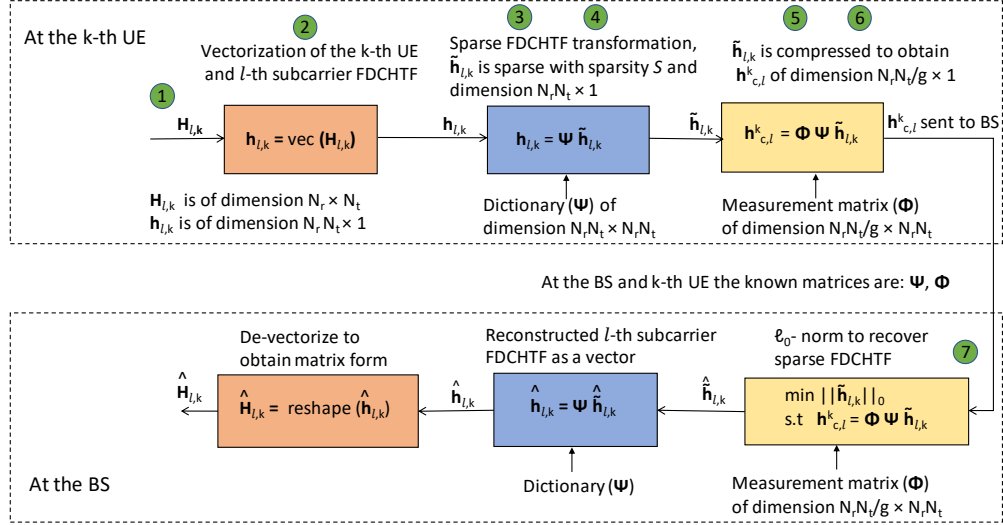


FIGURE 2: Overview of the considered CSI feedback compression scheme in the massive MU-MIMO-OFDM system. The FDCHTF across the l -th subcarrier of the k -th UE is compressed at the UE and reconstructed at the BS.

response (CIR) of the link spanning from the q -th BS antenna to the p -th UE antenna.

The spatial correlation of massive MIMO channels can be modeled by a Kronecker structure having separable transmit and receive correlation matrices [31], with $\bar{\mathbf{H}}_{n,k}$ given by

$$\bar{\mathbf{H}}_{i,k} = \frac{1}{\sqrt{\text{tr}(\mathbf{R}_{UE,k})}} \mathbf{R}_{UE,k}^{\frac{1}{2}} \check{\mathbf{H}}_{i,k} \mathbf{R}_{BS}^{\frac{1}{2}}, \quad (2)$$

where $\check{\mathbf{H}}_{i,k}$ is a $N_r \times N_t$ matrix whose elements are independent and identically distributed (i.i.d.) complex zero-mean, unit variance, Gaussian random entries. Furthermore, \mathbf{R}_{BS} and $\mathbf{R}_{UE,k}$ are the spatial correlation matrices at the BS and k -th UE, respectively.

The spatial correlation matrices are generated by Jakes' model often used in the literature, so the uv -th element of \mathbf{R}_{BS} and $\mathbf{R}_{UE,k}$, can be modeled by $r_{uv} = J_0(2\pi d_{uv}/\lambda)$ where d_{uv} is the distance between the antennas u and v , λ is the carrier wavelength and $J_0(\cdot)$ denotes the zeroth-order Bessel function of first kind [39].

B. Compressive Sensing Based Channel Reconstruction

Fig. 2 shows the basic schematic of the FDCHTF compression and reconstruction across the l -th subcarrier of the k -th UE. More specifically, observe in Fig. 3 that at the k -th UE we present the FDCHTF view across all the subcarriers and its sparsification using the existing as well as the proposed methods in parallel. The remainder of this section introduces each of the steps numbered in both figures.

① In between the BS and a k -th UE the complete channel frequency response matrix that includes all the N_c subcarrier channels is formed by stacking the channel matrices column-wise:

$$\mathbf{H}_k = [\mathbf{H}_{1,k}, \dots, \mathbf{H}_{l,k}, \dots, \mathbf{H}_{N_c,k}]. \quad (3)$$

② We assume that the k -th UE perfectly estimates its channel matrix \mathbf{H}_k , which should be shared with the BS through feedback. Instead of sending the FDCHTF of each subcarrier, the matrix $\mathbf{H}_{l,k}$ is vectorized first into an $N_r N_t \times 1$ column vector using the $\text{vec}(\cdot)$ operation

$$\mathbf{h}_{l,k} = \text{vec}(\mathbf{H}_{l,k}). \quad (4)$$

③ ④ In practical systems, the UE has to compress the estimated channel vector $\mathbf{h}_{l,k} \in \mathbb{C}^{N_r N_t \times 1}$ to avoid high feedback load. The wireless channel vector $\mathbf{h}_{l,k}$ can be represented by a sparse vector [31] after a transformation

$$\mathbf{h}_{l,k} = \Psi \tilde{\mathbf{h}}_{l,k}, \quad (5)$$

where $\tilde{\mathbf{h}}_{l,k}$ is the sparse representation of $\mathbf{h}_{l,k}$. The number of non-zero components of a sparse channel vector is called the sparsity or sparsity index, and it is denoted by S , while Ψ is a $N_r N_t \times N_r N_t$ dictionary known to both the UE and the BS. A popular example of Ψ is the DFT matrix. Next, we introduce the measurement (sensing) matrix Φ , which plays a crucial role in compressive sensing. The measurement (sensing) matrix defines the measurement process in CS, which influences the reconstruction quality and efficiency of the signal recovery algorithm. It is responsible for mapping the original high-dimensional signal to a lower-dimensional signal.

⑤ ⑥ To compress the channel vector $\mathbf{h}_{l,k}$, a measurement matrix $\Phi \in \mathbb{C}^{N_g \times N_r N_t}$ ($N_g \ll N_r N_t$) that satisfies the Restricted Isometry Property (RIP) [8], which facilitates sparse vector recovery relying on:

$$\mathbf{h}_{c,l}^k = \Phi \Psi \tilde{\mathbf{h}}_{l,k}, \quad (6)$$

where $\mathbf{h}_{c,l}^k$ is the compressed channel vector with dimension $N_g \times 1$. Let us now define $\Theta = \Phi \Psi$.

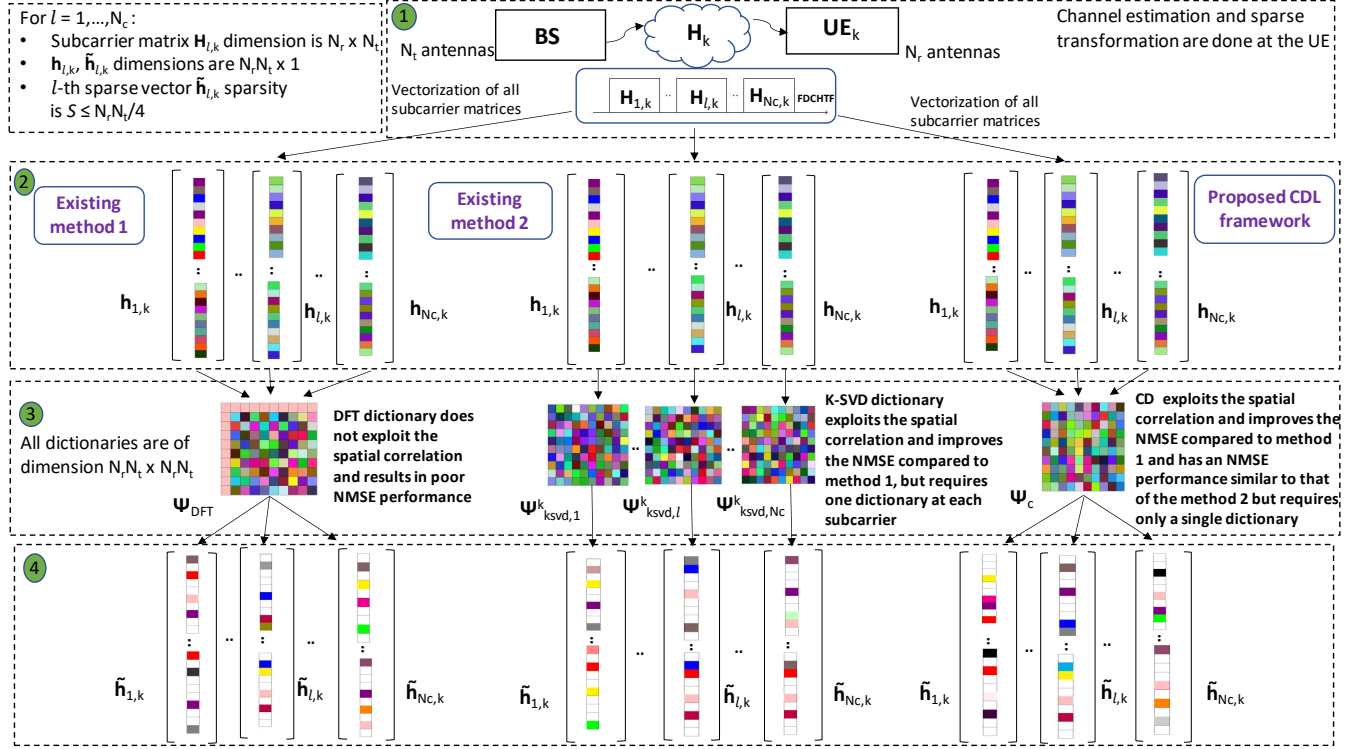


FIGURE 3: Overview of the massive MU-MIMO-OFDM system having a k -th UE with N_r RAs and a BS with N_t TAs. \mathbf{H}_k represents the complete FDCHTF at the k -th UE and $\mathbf{H}_{l,k}$ represents the FDCHTF across the l -th subcarrier of the k -th UE. The FDCHTFs are vectorized and then undergo sparse transformation using the dictionary obtained from the existing methods 1, 2 of [15] and the proposed framework. The circled numbers and the notations are the same as in Fig.2.

⑦ Then the reconstruction of $\mathbf{h}_{l,k}$ can be formulated as an ℓ_0 -norm minimization problem and the sparse vector $\tilde{\mathbf{h}}_{l,k}$ can be obtained by solving

$$\min_{\tilde{\mathbf{h}}_{l,k}} \|\tilde{\mathbf{h}}_{l,k}\|_0 \quad s.t. \quad \mathbf{h}_{c,l}^k = \Theta \tilde{\mathbf{h}}_{l,k}. \quad (7)$$

Thus, instead of feeding back $\mathbf{h}_{l,k}$, the UE sends a low-dimensional vector $\mathbf{h}_{c,l}^k$ to the BS for reducing the FDCHTF feedback. The BS reconstructs $\hat{\mathbf{h}}_{l,k}$ from $\mathbf{h}_{c,l}^k$, where $\hat{\mathbf{h}}_{l,k}$ represents the reconstructed $\mathbf{h}_{l,k}$. The reconstructed channel vector $\hat{\mathbf{h}}_{l,k}$ at the BS is utilized for precoding during the data transmission stage. The precoder matrices employed at the BS are denoted as \mathbf{W}^g and \mathbf{W}_{op}^g , which correspond to the beamforming weights. These weights are obtained from the true channels and the channels estimated using CDL-OP dictionary, respectively, for a compression factor of g . Here, the compression factor g is defined as $g = \frac{N_r N_t}{N_g}$, where $N_g \times 1$ represents the dimension of the compressed channel vector $\mathbf{h}_{c,l}^k$.

C. Motivation for the Common Dictionary Learning Framework

In CS-based feedback schemes, the traditional choice of the dictionary is a fixed DFT matrix, which does not exploit the spatial correlation between the antennas. The authors

of [11] proposed a rotated version of the DFT dictionary for better exploiting the sparsity, resulting in reduced FDCHTF mean-squared error (MSE) for a narrowband multi-user system supporting single antenna UEs. But this rotated basis still failed to exploit the antenna's spatial correlation for improving the MSE further.

The authors of [15] have shown that a dictionary can be learned using the K-SVD algorithm for narrowband FDD massive SU-MIMO systems. This K-SVD dictionary learned exploits the spatial correlation between the antennas, and its FDCHTF reconstruction performance is improved compared to the fixed DFT dictionary. The proposed method requires FDCHTF and dictionary feedback to the BS. However, in practical communication systems, the channels are frequency-selective, and OFDM is a ubiquitous technique for such systems. In a massive MU-MIMO-OFDM system, to extend the idea of dictionary learning, it is necessary to feed back the FDCHTF and K-SVD based dictionary of each subcarrier of all UEs. Feeding back the entire FDCHTF \mathbf{H}_k of the k -th subcarrier will be a huge burden in the uplink. Another important issue is that substantial memory is required for saving all the N_c subcarrier dictionaries at both the UE and the BS. The dimension of each subcarrier dictionary is $N_r N_t \times N_r N_t$, hence the memory required to store N_c dictionaries is $N_c (N_r N_t)^2$.

To overcome these challenges, we propose the novel idea of a common dictionary, which can replace the requirement of individual subcarrier dictionaries. The CD is designed for exploiting the spatial correlation across all the subcarriers and UEs in the FD, hence improving the CSI reconstruction accuracy. The proposed CD reduces the CSI feedback load and memory requirement in both single and multi-UE systems. In particular, the feedback load is further reduced for a single-UE system by sending only a single CD from the UE to the BS. Hence, the proposed CDL framework reduces the CSI feedback and memory requirements, and we also study the NMSE performance compared to the DFT and subcarrier K-SVD dictionaries.

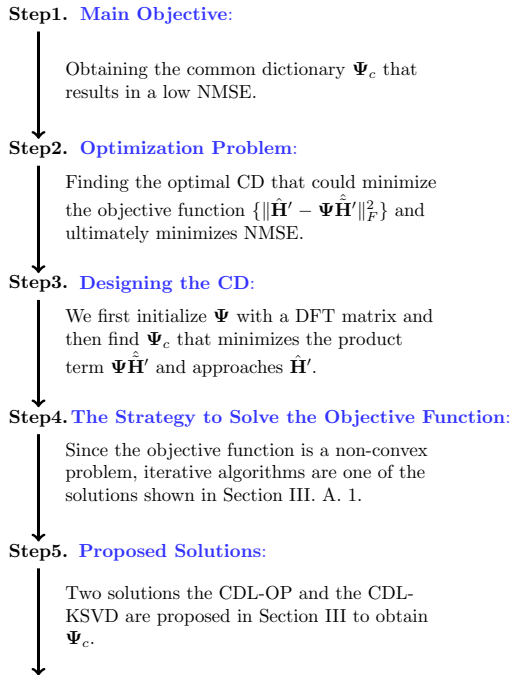


FIGURE 4: Flow of the mathematical analysis.

III. Proposed Common Dictionary Learning Framework

In this section, we detail the CDL framework proposed for a multi-UE system that constructs a dictionary from the estimated channel vectors and K-SVD based dictionaries of UEs. Before introducing the framework proposed, in Fig. 4 we provided a diagram showing the flow of the analysis described in the paper. This diagram guides the reader through the paper.

A. Common Dictionary Learning Framework

The main goal of the proposed CDL framework is to construct a CD, denoted by Ψ_c , that can exploit the correlation of channels across all the UEs and BS, for improving the CSI reconstruction at the BS. The matrix of training channel vectors is denoted by \mathbf{H}' , which consists of M'

channel vectors collected for N different frames across N_c subcarriers and K UEs. Then we have $M' = N \times N_c \times K$.

To elaborate further, \mathbf{H}' is structured as $\mathbf{H}' = [\mathbf{H}'_1, \dots, \mathbf{H}'_k, \dots, \mathbf{H}'_K]$, and each sub-matrix in \mathbf{H}' is represented as $\mathbf{H}'_k = [\mathbf{H}'_{1,k}, \dots, \mathbf{H}'_{l,k}, \dots, \mathbf{H}'_{N_c,k}] \forall k \in \{1, 2, \dots, K\}, \forall l \in \{1, 2, \dots, N_c\}$. Similarly, $\mathbf{H}'_{l,k}$ is defined as $\mathbf{H}'_{l,k} = [\mathbf{h}_{l_1,k}, \dots, \mathbf{h}_{l_n,k}, \dots, \mathbf{h}_{l_N,k}]$, where $\mathbf{h}_{l_n,k}$ represents the channel vector transformation of $\mathbf{H}_{l_n,k}$ at the n -th MU-MIMO-OFDM frame (time-instant). We assume that the channel envelope remains constant for an OFDM frame and then changes for the successive frames, according to the vehicular velocity. Hence the consecutive frames are correlated.

The sparse representation of the matrix \mathbf{H}' is denoted as $\tilde{\mathbf{H}}' = [\tilde{\mathbf{H}}'_1, \dots, \tilde{\mathbf{H}}'_{k_1}, \dots, \tilde{\mathbf{H}}'_{K'}]$, and each sub-matrix in $\tilde{\mathbf{H}}'$ is represented as $\tilde{\mathbf{H}}'_k = [\tilde{\mathbf{H}}'_{1,k}, \dots, \tilde{\mathbf{H}}'_{l,k}, \dots, \tilde{\mathbf{H}}'_{N_c,k}] \forall k \in \{1, 2, \dots, K\}, \forall l \in \{1, 2, \dots, N_c\}$. Similarly $\tilde{\mathbf{H}}'_{l,k} = [\tilde{\mathbf{h}}_{l_1,k}, \dots, \tilde{\mathbf{h}}_{l_n,k}, \dots, \tilde{\mathbf{h}}_{l_N,k}]$, where $\tilde{\mathbf{h}}_{l_n,k}$ denotes the sparse representation of the channel vector $\mathbf{h}_{l_n,k}$.

The CDL optimization problem is formulated as:

$$\begin{aligned} \min_{\Psi, \tilde{\mathbf{H}}'} \{ \|\mathbf{H}' - \Psi \tilde{\mathbf{H}}'\|_F^2 \} \\ \text{s.t. } \|\tilde{\mathbf{h}}_{l_n,k}\|_0 \leq S, \forall n \in \{1, 2, \dots, N\}, \\ \forall l \in \{1, 2, \dots, N_c\}, \forall k \in \{1, 2, \dots, K\}. \end{aligned} \quad (8)$$

To solve the optimization problem in (8) we propose the following methods.

1) CDL-KSVD method:

In the CDL-KSVD method the training set \mathbf{H}' consists of the channel vectors of all the UEs. The training set is employed to learn the dictionary Ψ_c using the K-SVD algorithm [36]. The K-SVD algorithm has two stages: the sparse coding stage and the dictionary update stage. In the sparse coding stage, each column of \mathbf{H}' is sparsely represented using a dictionary. The dictionary update stage involves updating each column of Ψ with a dominant singular vector. As a result, the learned dictionary Ψ_c has unit-norm columns.

- *Sparse coding stage:* In the first stage of the K-SVD algorithm, the optimization problem is formulated as:

$$\begin{aligned} \min_{\tilde{\mathbf{H}}'} \{ \|\mathbf{H}' - \Psi \tilde{\mathbf{H}}'\|_F^2 \} \\ \text{s.t. } \|\tilde{\mathbf{h}}_{l_n,k}\|_0 \leq S, \forall n \in \{1, 2, \dots, N\}, \\ \forall l \in \{1, 2, \dots, N_c\}, \forall k \in \{1, 2, \dots, K\}. \end{aligned} \quad (9)$$

To solve (9), we begin by initializing the matrix Ψ with a DFT dictionary. The next step involves finding the matrix \mathbf{H}' having a sparse representation, which is an ℓ_0 problem and it is carried out by using the OMP algorithm [8]. The objective of the OMP algorithm is to find a sparse representation of \mathbf{H}' using a small number of non-zero elements in the matrix $\tilde{\mathbf{H}}'$.

- *Dictionary update stage*: In the second stage of the K-SVD algorithm, the optimization problem is formulated as:

$$\min_{\Psi} \{ \|\mathbf{H}' - \Psi \hat{\mathbf{H}}'\|_F^2 \}. \quad (10)$$

The solution to the problem posed in (10) is obtained by updating each column of the dictionary by computing a partial SVD of a matrix [6]. After the dictionary update stage, the dictionary Ψ gets updated to Ψ_c . It is to be noted that this method updates only the columns corresponding to sparse coefficients of the channel matrix $\hat{\mathbf{H}}'$.

- Repeat sparse coding and dictionary update stages until the stopping criterion is met.

The main advantage of the CDL-KSVD method is that it captures the spatial correlation of the channel vectors. But its drawback is that it requires a partial SVD operation for each column update in the dictionary update stage, which is computationally expensive.

2) CDL-OP method:

The CDL-OP method stands for common dictionary learning - orthogonal Procrustes method. In this method we solve the orthogonal Procrustes problem to learn the CD [37]. The CD obtained is a square matrix with dimensions $N_r N_t \times N_r N_t$. The constraint imposed is that the columns of the dictionary should be orthogonal. The optimization problem is formulated as:

$$\min_{\Psi} \{ \|\mathbf{H}' - \Psi \hat{\mathbf{H}}'\|_F^2 \} \quad s.t. \quad \Psi^H \Psi = \mathbf{I}, \quad (11)$$

where Ψ in (11) may be found explicitly by singular value decomposition (SVD).

$$\begin{aligned} \text{Let } \mathbf{C} &= \hat{\mathbf{H}}' \mathbf{H}'^H \\ [\mathbf{U}, \Sigma, \mathbf{V}] &= \text{SVD}(\mathbf{C}) \\ \Psi &= \mathbf{V} \mathbf{U}^H. \end{aligned} \quad (12)$$

The resulting dictionary Ψ obtained in (12) is the CD (Ψ_c). The main advantage of the CDL-OP method is that it captures the spatial correlation of the channel vectors, but at the cost of an SVD operation.

B. Common Dictionary for Wideband Multi-UE System

A wideband channel has a broader signal bandwidth than the coherence bandwidth. In this section, we first discuss the CDL framework conceived for a wideband system supporting K UEs, and then highlight the simplified scenario, where a single UE is present. Next, we will quantify the memory savings of storing only a single CD. Then in the final subsection, we elaborate on the dictionary feedback reduction by sending only a single CD in a single-UE system.

In the multi-UE system, since no communication takes place among the K UEs, CDL is impossible at any UE. Consequently, the CDL is only feasible at the BS. For

the CDL at the BS, we require the subcarrier dictionaries and the reconstructed channels (used as training channel vectors). Let the reconstructed sparse channel matrix at the BS be represented by $\hat{\mathbf{H}}' = [\hat{\mathbf{H}}'_1, \dots, \hat{\mathbf{H}}'_k, \dots, \hat{\mathbf{H}}'_K]$, where each sub-matrix in $\hat{\mathbf{H}}'$ is represented as $\hat{\mathbf{H}}'_k = [\hat{\mathbf{H}}'_{1,k}, \dots, \hat{\mathbf{H}}'_{l,k}, \dots, \hat{\mathbf{H}}'_{N_c,k}] \quad \forall k \in \{1, 2, \dots, K\}$, with $\hat{\mathbf{H}}'_{l,k} = [\hat{\mathbf{h}}_{l_1,k}, \dots, \hat{\mathbf{h}}_{l_n,k}, \dots, \hat{\mathbf{h}}_{l_N,k}]$, containing N reconstructed sparse channel vectors of each subcarrier, i.e., $\forall l \in \{1, 2, \dots, N_c\}$.

Let the reconstructed matrix of training channel vectors at the BS be represented by $\hat{\mathbf{H}}' = [\hat{\mathbf{H}}'_1, \dots, \hat{\mathbf{H}}'_k, \dots, \hat{\mathbf{H}}'_K]$, where each sub-matrix in $\hat{\mathbf{H}}'$ is represented as $\hat{\mathbf{H}}'_k = [\hat{\mathbf{H}}'_{1,k}, \dots, \hat{\mathbf{H}}'_{l,k}, \dots, \hat{\mathbf{H}}'_{N_c,k}] \quad \forall k \in \{1, 2, \dots, K\}$, with $\hat{\mathbf{H}}'_{l,k} = [\hat{\mathbf{h}}_{l_1,k}, \dots, \hat{\mathbf{h}}_{l_N,k}]$ when considering N reconstructed channel vectors for each subcarrier i.e., $\forall l \in \{1, 2, \dots, N_c\}$. The total number of reconstructed training channel vectors in $\hat{\mathbf{H}}'$ is $M' = N \times N_c \times K$.

Importantly, at this stage we have to consider $\hat{\mathbf{H}}'$ instead of \mathbf{H}' and $\hat{\mathbf{H}}'$ instead of $\hat{\mathbf{H}}$ in (8). The optimization problem of finding Ψ_c in the multi-UE system is formulated as follows:

$$\begin{aligned} \min_{\Psi, \hat{\mathbf{H}}'} \{ \|\hat{\mathbf{H}}' - \Psi \hat{\mathbf{H}}'\|_F^2 \} \\ s.t. \quad \|\hat{\mathbf{h}}_{l_n,k}\|_0 \leq S, \quad \forall n \in \{1, 2, \dots, N\}, \\ \forall l \in \{1, 2, \dots, N_c\}, \quad \forall k \in \{1, 2, \dots, K\}. \end{aligned} \quad (13)$$

The single-UE system ($K = 1$) is a special case of a multi-UE system. For the current system when compared to the multi-UE system of Fig. 5 there is no need to send the subcarrier dictionaries ($\Psi_{k_{svd},l}^k, \forall n \in \{1, 2, \dots, N\}, \forall l \in \{1, 2, \dots, N_c\}$) from the UEs to the BS. The CD is learned at the UE itself using one of the two proposed methods and then the UE sends Ψ_c to the BS. Now both the BS and the UE will start using Ψ_c . The total number of training channel vectors in \mathbf{H}' is $M' = N \times N_c$.

The optimization problem of finding Ψ_c is as follows:

$$\begin{aligned} \min_{\Psi, \hat{\mathbf{H}}'} \{ \|\mathbf{H}' - \Psi \hat{\mathbf{H}}'\|_F^2 \} \\ s.t. \quad \|\tilde{\mathbf{h}}_{l_n}\|_0 \leq S, \quad \forall n \in \{1, 2, \dots, N\}, \\ \forall l \in \{1, 2, \dots, N_c\}. \end{aligned} \quad (14)$$

The CDL framework of our multi-UE system is outlined in Algorithm 1 and its block diagram is shown in Fig. 5. More specifically, in the Algorithm 1 we present the step-by-step procedure of the CDL framework. The remainder of this sub-section introduces each of the steps numbered in the Fig. 5 and the corresponding steps in the algorithm.

① The BS sends the pilots to all the K -UEs in the system and each UE estimates its channels and follows the steps 4 to 10 in the algorithm for N frames and learns the K-SVD based subcarrier dictionaries.

② Each UE sends the N_c K-SVD dictionaries to the BS. For the next N frames each UE compresses the l -th

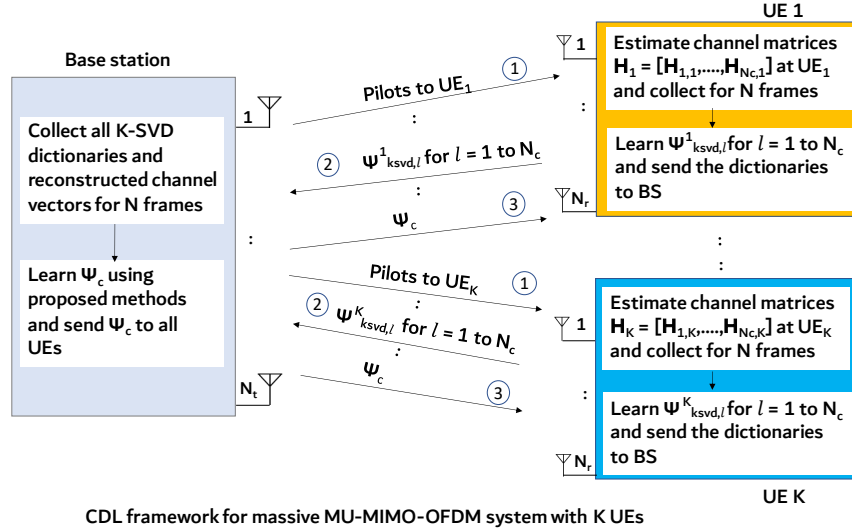


FIGURE 5: Overview of the CDL framework for FDD massive MU-MIMO-OFDM system. Right: K UEs with N_r receive-antennas each; Left: massive MIMO base station with N_t transmit antennas; Center: For simplicity, only dictionary feedback is shown.

subcarrier FDCHTF using the K-SVD dictionary ($\Psi_{ksvd,l}^k$) and sends it to the BS. Then the BS reconstructs the l -th subcarrier FDCHTF with the aid of the same K-SVD dictionary. Using the reconstructed FDCHTFs and the K-SVD based subcarrier dictionaries of all the K UEs, the BS learns the Ψ_c . The ② procedure corresponds to the steps 14 to 19 in the algorithm.

③ After learning the CD at the BS, the BS sends the CD to all the K -UEs, the UEs and the BS will follow the steps 22 to 25 in the algorithm for FDCHTF compression and reconstruction using Ψ_c .

1) Memory Reduction Calculation:

- The memory required to store each subcarrier dictionary $\Psi_{ksvd,l}^k$ is $(N_r N_t)^2$, $\forall l \in \{1, 2, \dots, N_c\}, \forall k \in \{1, 2, \dots, K\}$.
- The total memory required to store N_c subcarrier dictionaries is $N_c(N_r N_t)^2$.
- The memory required to store Ψ_c is $(N_r N_t)^2$.
- Total memory storage reduction for a K -UE system = $K \times ([\text{Memory required to store } N_c \text{ subcarrier dictionaries}] - [\text{Memory required to store } \Psi_c])$, which is formulated as:

$$\Delta_{saved} = K(N_c - 1)(N_r N_t)^2. \quad (15)$$

- The total memory storage reduction for a single-UE is

$$\Delta_{saved} = (N_c - 1)(N_r N_t)^2. \quad (16)$$

2) Dictionary Feedback Reduction Calculation by Sending a CD in a Single-UE System:

- The dimension of each subcarrier K-SVD dictionary $\Psi_{ksvd,l}$ is $N_r N_t \times N_r N_t$, $\forall l \in \{1, 2, \dots, N_c\}$.

- The total dimension of N_c subcarrier dictionaries is $N_c \times N_r N_t \times N_r N_t$.
- The dimension of Ψ_c is $N_r N_t \times N_r N_t$.
- Total dictionary feedback reduction for a single-UE (\mathcal{T}_{saved}) = [Feedback required for sending N_c subcarrier dictionaries (\mathcal{T}_{ksvd})] – [Feedback required for sending Ψ_c (\mathcal{T}_{com})], where we have

$$\mathcal{T}_{ksvd} = N_c(N_r N_t)^2$$

$$\mathcal{T}_{com} = (N_r N_t)^2$$

$$\mathcal{T}_{saved} = \mathcal{T}_{ksvd} - \mathcal{T}_{com} = (N_c - 1)(N_r N_t)^2.$$

- *Reduction in dictionary feedback:* We define the feedback reduction factor by (Υ):

$$\Upsilon = \frac{\mathcal{T}_{com}}{\mathcal{T}_{ksvd}} = \frac{1}{N_c} \quad (17)$$

TABLE 5: Dictionary feedback reduction factor in a single-UE System.

| N_t | N_r | N_c | \mathcal{T}_{ksvd} | \mathcal{T}_{com} | Υ |
|-------|-------|-------|----------------------|---------------------|------------|
| 64 | 1 | 4 | 16384 | 4096 | 1/4 |
| 64 | 1 | 32 | 131072 | 4096 | 1/32 |

3) Computational Complexity of the Algorithm:

We calculate the computational complexity of the dictionary learning stage for both the CDL-OP and the CDL-KSVD methods.

a) CDL-OP method:

- In (12), the SVD operation requires all the eigenvectors, resulting in a full SVD operation.

Algorithm 1: CDL Framework for K Users**Input:** Ψ_{DFT} , Pilots**Output:** Ψ_c

1 **Variables:** Frame index n , UE index k , subcarrier index l .

2 **Implementation:** $\forall k \in \{1, \dots, K\}, \forall l \in \{1, \dots, N_c\}$

3 **for** $n = 1$ **to** $2N$ **do**

4 BS transmits pilot sequences for UE₁ to UE_K.

5 The k -th UE estimates its channel matrix $\mathbf{H}_{l_n,k}$ across l -th subcarrier from the pilots.

6 After transformatation of $\mathbf{H}_{l_n,k}$ to vector $\mathbf{h}_{l_n,k}$, k -th UE at l -th subcarrier computes its compressed vector \mathbf{h}_{c,l_n}^k using $\mathbf{h}_{l_n,k}$, $\tilde{\mathbf{h}}_{l_n,k}$, Ψ_{DFT} and sends \mathbf{h}_{c,l_n}^k to BS.

7 BS reconstructs $\hat{\mathbf{h}}_{l_n,k}$ and $\hat{\mathbf{h}}_{l_n,k}$ using Ψ_{DFT} and \mathbf{h}_{c,l_n}^k . BS uses $\hat{\mathbf{h}}_{l_n,k}$ for precoding.

8 In parallel k -th UE at l -th subcarrier collects training channel vectors $\mathbf{h}_{l_n,k}$'s to form matrix $[\mathbf{h}_{l_1,k}, \dots, \mathbf{h}_{l_N,k}]$.

9 **if** $n = N$ **then**

10 The k -th UE learns $\Psi_{ksvd,l}^k$ from $[\mathbf{h}_{l_1,k}, \dots, \mathbf{h}_{l_N,k}]$ and Ψ_{DFT} using K-SVD algorithm and sends $\Psi_{ksvd,l}^k$ (once) to BS.

11 **end**

12 **end**

13 **for** $n = N + 1$ **to** $2N$ **do**

14 Follow steps 4 and 5 for another N frames.

15 The k -th UE at l -th subcarrier computes compressed vector \mathbf{h}_{c,l_n}^k using $\mathbf{h}_{l_n,k}$, $\tilde{\mathbf{h}}_{l_n,k}$, $\Psi_{ksvd,l}^k$ and sends \mathbf{h}_{c,l_n}^k to BS.

16 BS reconstructs $\hat{\mathbf{h}}_{l_n,k}$, $\hat{\mathbf{h}}_{l_n,k}$ using $\Psi_{ksvd,l}^k$, \mathbf{h}_{c,l_n}^k .

17 **if** $n = 2N$ **then**

18 BS computes Ψ_c using one of the two methods from $\hat{\mathbf{h}}_{l_n,k}$'s, $\tilde{\mathbf{h}}_{l_n,k}$'s and $\Psi_{ksvd,l}^k$ of all UEs and sends Ψ_c to all the UEs.

19 **end**

20 **end**

21 **for** $i > 2N$ **do**

22 Follow steps 4 and 5

23 The k -th UE starts using Ψ_c instead of $\Psi_{ksvd,l}^k$ for step 15 and sends compressed vector \mathbf{h}_{c,l_n}^k to BS.

24 BS reconstructs $\hat{\mathbf{h}}_{l_n,k}$ and $\hat{\mathbf{h}}_{l_n,k}$ of k -th UE using Ψ_c and \mathbf{h}_{c,l_n}^k (obtained from step 23).

25 BS uses $\hat{\mathbf{h}}_{l_n,k}$ of each UE for precoding.

26 **end**

- The computation of a full SVD operation, specifically using the Golub-Reinsch SVD (GR-SVD) method, requires $21(N_r N_t)^3$ floating-point operations

(FLOPS) [6]. On the other hand, the Chan-SVD (R-SVD) method requires $26(N_r N_t)^3$ FLOPS [6].

- Therefore, to update the dictionary, we require a computational complexity of $\mathcal{O}[(N_r N_t)^3]$.

b) CDL-KSVD method:

- In (10), updating each column of the dictionary requires an SVD operation. This SVD operation only requires the dominant eigenvector, resulting in a partial SVD computation.
- The GR-SVD method requires $14N_r N_t N_c'^2 + 9N_c'^3$ FLOPS [6], while the R-SVD method requires $6N_r N_t N_c'^2 + 20N_c'^3$ FLOPS [6]. Here, N_c' represents the number of non-zero coefficients corresponding to the k -th row in $\tilde{\mathbf{H}}'$, and N_c' ranges from 0 to M' .
- Therefore, to update the complete dictionary, a total of $N_r N_t$ partial SVD operations are required.

c) For example, let us consider $N_t = 64$, $N_r = 1$, $M' = 1600$, and an average value of $N_c' = M'/4$. The computational complexity in FLOPS is provided in Table 6. We represent the number of FLOPS required for updating a single column in the dictionary by CDL-KSVD (min), and that imposed by updating all columns in the dictionary using CDL-KSVD (max).

TABLE 6: Computational complexity in FLOPS

| Method | GR-SVD | Chan-SVD |
|----------------|--------------------|--------------------|
| CDL-OP | $5.505 * 10^6$ | $6.8157 * 10^6$ |
| CDL-KSVD (min) | $7.1936 * 10^8$ | $1.3414 * 10^9$ |
| CDL-KSVD (max) | $4.6039 * 10^{10}$ | $8.5852 * 10^{10}$ |

4) CSI Feedback Case Study in a Single UE:

The dimension of the compressed channel vector $\mathbf{h}_{c,l}^k$ ($\in \mathbb{C}^{N_g \times 1}$) sent from the UE in the uplink can be varied by adjusting the compression factor g . Specifically, the dimension is given by $N_g = \frac{N_r N_t}{g}$. By tuning the value of g , we can beneficially reduce the amount of CSI feedback required.

To quantify the feedback requirements, we introduce the variables γ_u and γ_c to represent the feedback for the non-dictionary and dictionary-based methods, respectively. In a non-dictionary based method without compression, the CSI fed back from the UE corresponds to $N_c N_r N_t$ elements for one frame. For N' frames the CSI feedback will be $\gamma_u = N' N_c N_r N_t$. However, in a dictionary-based method associated with compression, the feedback is constituted by the CSI information having $\frac{N_c N_r N_t}{g}$ elements for one frame, along with a one-time transmission of a dictionary with $(N_r N_t)^2$ elements. So, for a total of N' frames the feedback is given by $\gamma_c = (N_r N_t)^2 + \frac{N' N_c N_r N_t}{g}$.

We define Γ as the CSI feedback ratio, which is calculated as the ratio between γ_c and γ_u . If $\Gamma < 1$, it indicates that the value of γ_c is lower than γ_u , resulting in a saving in CSI

feedback.

$$\Gamma = \frac{\gamma_c}{\gamma_u} = \frac{(N_r N_t)^2 + \frac{N' N_c N_r N_t}{g}}{N' N_c N_r N_t} = \frac{N_r N_t}{N' N_c} + \frac{1}{g} \quad (18)$$

For example in Table 7 we consider a scenario associated with $N' = 2^{10}$ and vary the values of N_c , N_r , and g . Using the formula given in 18, we demonstrate significant reductions in CSI feedback. The level of compression applied to the channel vector $\mathbf{h}_{c,l}^k$ depends on the sparsity parameter S . As per the lower bound, the number of elements in $\mathbf{h}_{c,l}^k$ must satisfy $N_g > 2S$ [9]. In Fig. 13, we illustrate the impact of the compression factor g on the BER vs. signal-to-noise ratio (SNR) performance for both the non-dictionary and dictionary-based methods.

TABLE 7: CSI feedback savings comparison table for $N' = 2^{10}$.

| g | N_c | N_t | N_r | $\Gamma = \frac{\gamma_c}{\gamma_u}$ |
|-----|-------|-------|-------|--------------------------------------|
| 2 | 32 | 64 | 1 | 0.5 |
| 2 | 64 | 64 | 2 | 0.5 |
| 4 | 32 | 64 | 1 | 0.252 |
| 4 | 64 | 64 | 2 | 0.252 |

IV. Numerical Results

In this section, we provide the simulation results for characterising the NMSE performances of the DFT dictionary (Ψ_{DFT}), of the individual K-SVD based subcarrier dictionaries ($\Psi_{ksvd,l}^k$) and of the proposed CD (Ψ_c). Using the DFT dictionary as the initial reference dictionary, we obtain the individual K-SVD based subcarrier dictionaries. Then Ψ_c is learned by the proposed methods. For NMSE calculations, each dictionary is used for reconstructing the P channel vectors of each subcarrier at the BS.

The NMSE of the reconstructed channel is used as a performance metric defined as

$$\text{NMSE} = \frac{1}{P} \sum_{i=1}^P \frac{\|\hat{\mathbf{h}}_{l_n,k} - \mathbf{h}_{l_n,k}\|_2^2}{\|\mathbf{h}_{l_n,k}\|_2^2}, \quad (19)$$

where $\hat{\mathbf{h}}_{l_n,k}$ is the reconstructed channel vector and $\mathbf{h}_{l_n,k}$ is the original one.

A. Simulation Settings

The simulations are carried out for a massive MIMO-OFDM system having $N_t = 64$, antenna spacing of $d = \lambda/15$, carrier wavelength λ , operating at a carrier frequency of $f_c = 2$ GHz. Furthermore, we have a communication bandwidth of $B = 20$ MHz, $K = 1$ and $K = 3$ UEs, $N = 50$, $P = 500$ test channel vectors, $N_c = 32$ and $M = N_r N_t / 2$. For $M = 32$, all the existing and the proposed dictionaries reduce the CSI feedback by 50% in the uplink. For all the experiments, the subcarrier K-SVD based dictionaries are learned for $N = 50$ from each subcarrier.

For experiments in the multi-UE system, the channels are generated using a Quasi Deterministic Radio Channel

Generator (QuaDRiGa) [40], [41] for the three UEs having velocities of $V = 10, 15$ and 20 kmph. For experiments in the single-UE system, the channels are taken from the UE of $V = 20$ kmph. The channel update rate (CUR) considered to generate channels in QuaDRiGa is 10 ms. The QuaDRiGa simulation platform is recommended by 3GPP (3rd Generation Partnership Project) for designing and simulating wireless communications systems.

The main motivation for the CDL is not only to reduce the CSI feedback but also to reduce the CSI reconstruction NMSE. The benefit of the proposed methods in terms of the NMSE performance has to be studied. Hence we have conducted experiments for determining which of the proposed methods will best replace the DFT dictionary and subcarrier K-SVD based dictionaries in both single-UE and multi-UE systems. Since we have considered $N_c = 32$, it is not feasible to show the CD performance across all the subcarriers. In the single-UE system, we have considered subcarriers $l = 1$ or 8 , since the channel gains of these two subcarriers are relatively low over the period of time. In the multi-UE system, we have considered the first subcarrier $l = 1$ of all three UEs to evaluate the NMSE performance as a function of sparsity and compared the proposed methods' CD performance to the DFT and K-SVD dictionaries in the literature.

In OFDM systems, the need for subcarrier K-SVD based dictionaries increases with the number of subcarriers. The FDCHTFs of each subcarrier are considered to be independent in a wideband OFDM system, but this is only realistic for extremely long CIRs. Hence in the proposed system we assume having realistic correlation among subcarriers in the FD. This correlation among the subcarriers is captured by the CD using one of the two proposed methods. Our CDL procedure may also be extended to larger N_c .

In all the simulation results, for each subcarrier it can be observed that the NMSE decreases as the sparsity increases. This is because in the sparse vector transformation (5) the sparse vector $\tilde{\mathbf{h}}$ picks many columns in the dictionary for higher sparsities, which in turn helps to solve the optimization problem (7) by minimizing the distance between \mathbf{h} and $\tilde{\mathbf{h}}$. Hence, higher sparsity will improve the reconstruction performance.

Experiment 1. *In this single-UE experiment, we study the NMSE performance across a particular subcarrier of the UE using the CD learned from the proposed methods and existing methods as a function of sparsity. The proposed methods' CD is learned across all the subcarriers of the UE. For this experiment we consider a massive SU-MIMO-OFDM system having $N_c = 32$ subcarriers and a UE having $N_r = 1$ RA and moving with a velocity of 20 kmph.*

In Fig. 6, we consider the subcarrier $l = 1$ to study the NMSE performance of all the dictionaries. For a particular sparsity index of $S = 8$, the NMSE of the CDL-KSVD dictionary is 1.7×10^{-2} , of the CDL-OP dictionary is

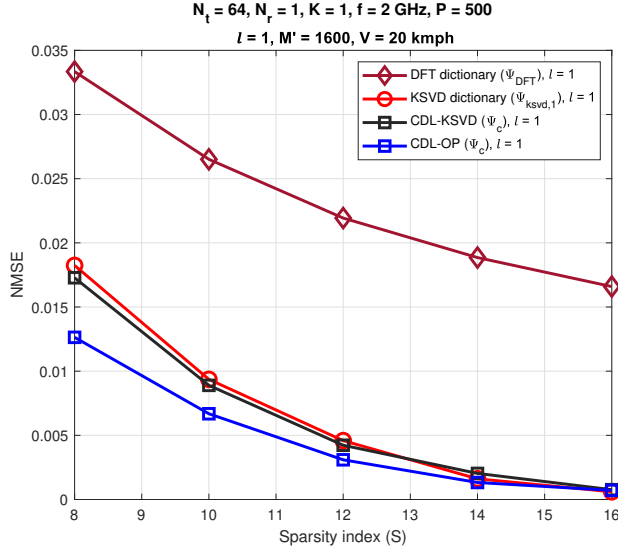


FIGURE 6: A single-UE system is considered, where the NMSE performance comparison among all the dictionaries is carried out for $N_t = 64$, $N_r = 1$ and $N_c = 32$. Subcarrier 1 is considered for comparison and the UE velocity is 20 kmph.

1.3×10^{-2} , of the subcarrier K-SVD based dictionary is 1.8×10^{-2} , and of the DFT dictionary is 3.3×10^{-2} . The CDL-OP dictionary has the lowest NMSE at $S = 8$. For all other sparsities, the CDL-OP and the CDL-KSVD method dictionaries perform similarly, and the NMSE values are close to those of the subcarrier K-SVD dictionary. All the proposed methods' CD exhibit better performance than the DFT dictionary.

In Fig. 7, we consider a scenario where the BS has a different number of antennas, namely $N_t = 16, 32$, and 64 . We consider the subcarrier $l = 1$ to study the NMSE performance of the CDL-OP dictionaries learned for different N_t values. We observe that the NMSE value increases with the number of antennas at the BS.

Experiment 2. In this single-UE experiment, we study the NMSE performance across different subcarriers of the UE employing the CD learned by the proposed methods and the individual subcarrier K-SVD based dictionaries as a function of sparsity. For this experiment we consider a massive SU-MIMO-OFDM system having $N_c = 32$ subcarriers. The UE is equipped with $N_r = 1$ (and 2) RAs and is moving at a velocity of 20 kmph.

In Fig. 8, the Ψ_c employed for NMSE characterization is learned from the CDL-KSVD method and in Fig. 9, the Ψ_c employed for NMSE characterization is learned from the CDL-OP method. Observe from Figs. 8 and 9, for subcarriers $l = 1$ and 8 at all the sparsity index values, the NMSE values are close to each other, but the CDL-OP method is the best among all the three methods in terms of the NMSE performance attained. Both the CDL-KSVD and CDL-OP

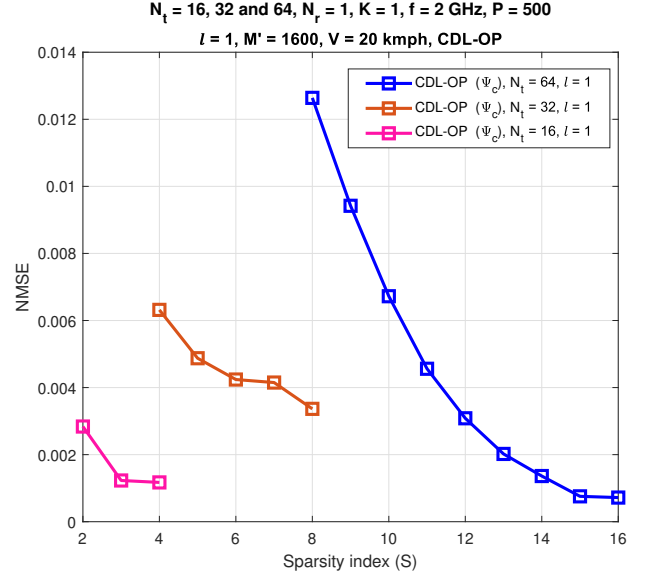


FIGURE 7: A single-UE system is considered, where the NMSE performance comparison among the CDL-OP dictionaries is carried out for $N_t = 16, 32$ and 64 , $N_r = 1$ and $N_c = 32$. Subcarrier 1 is considered for comparison and the UE velocity is 20 kmph.

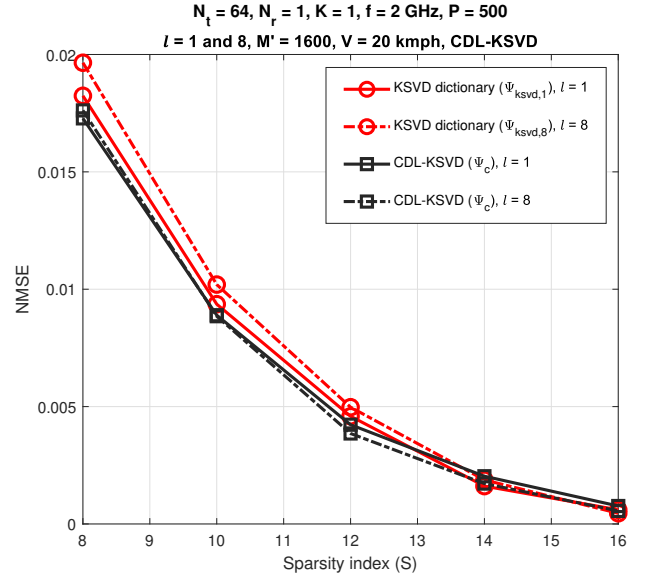


FIGURE 8: A single-UE system is considered, where the NMSE performance of the K-SVD dictionary and the CDL-KSVD dictionary are used for $N_t = 64$, $N_r = 1$ and $N_c = 32$. Subcarriers 1 and 8 are considered for comparison and the UE velocity is 20 kmph.

methods rely on the SVD operation and learn the CD from the channels estimated at the UE. Consequently, the NMSE reconstruction results shown in Figs. 8 and 9 exhibit a high degree of similarity.

We have carried out a simulation and presented the results in Fig. 10, where we specifically focus on the scenario where

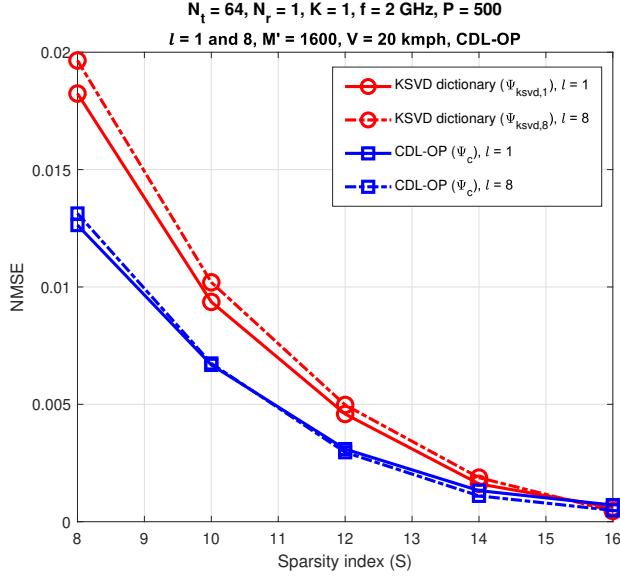


FIGURE 9: A single-UE system is considered, where the NMSE performance of the K-SVD dictionary and the CDL-OP dictionary are used for for $N_t = 64$, $N_r = 1$ and $N_c = 32$. Subcarriers 1 and 8 are considered for comparison and the UE velocity is 20 kmph.

$N_r > 1$, indicating the presence of multiple receive antennas. By considering this scenario, we ensure that our analysis is not limited to a specific number of receive antennas. It is observed that all the proposed methods' CD exhibit better NMSE performance than the DFT dictionary.

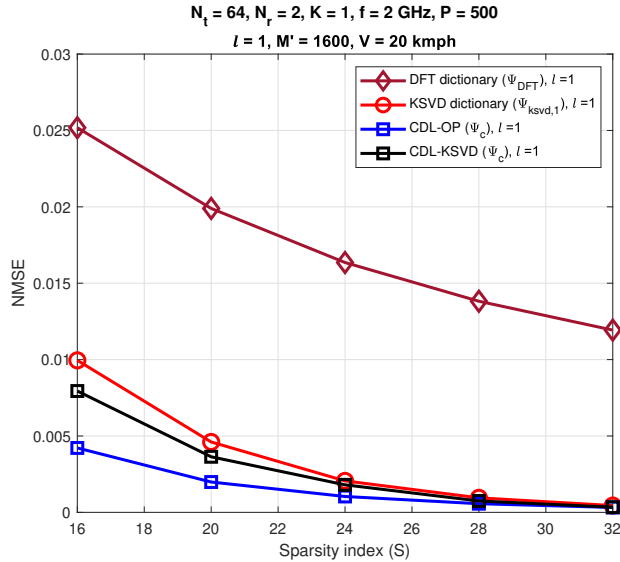


FIGURE 10: A single-UE system with multiple UE antennas is considered, where the NMSE performance comparison among all the dictionaries is carried out for $N_t = 64$, $N_r = 2$ and $N_c = 32$. Subcarrier 1 is considered for comparison and the UE velocity is 20 kmph.

Experiment 3. In this multi-UE experiment, we initially study the NMSE performance of the dictionary generated using the CDL-OP method and existing methods for a particular UE's subcarrier as a function of sparsity. Then we study the NMSE performance of the CDL-OP dictionary across different UEs for a particular subcarrier. The CDL-OP dictionary is learned across all the subcarriers and all the K UEs. For the experiment, we consider a massive MU-MIMO-OFDM system having $N_c = 32$ subcarriers and $K = 3$ UEs each associated with $N_r = 1$ RA.

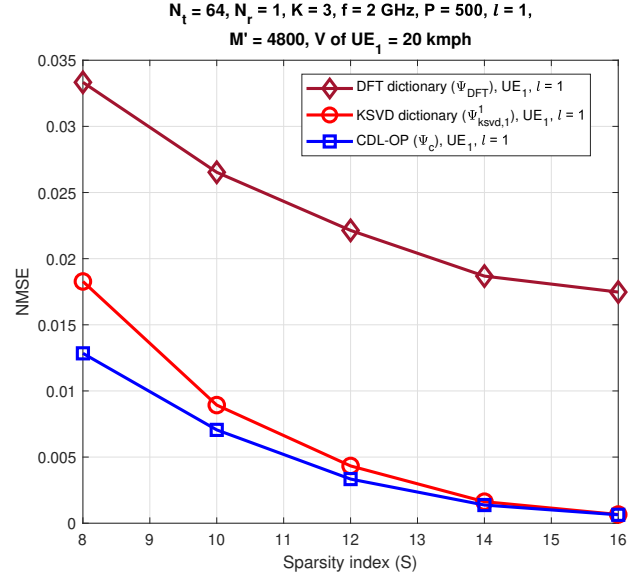


FIGURE 11: A multi-UE system is considered, where the NMSE performance comparison of the DFT, the K-SVD and the CDL-OP methods is carried out for $K = 3$, $N_t = 64$, $N_r = 1$ and $N_c = 32$. Subcarrier 1 of UE₁ is considered for comparison. The velocities of the three UEs are 10, 15, and 20 kmph.

The wireless channels are generated for three UEs having velocities of $V = 10, 15$, and 20 kmph using a QuaDRiGa simulator. Let us assume that a UE changes its velocity to that of another UE, but experiences different channel characteristics. In that case, there is no need to learn a new dictionary for that particular UE. The CD has already captured all the three UE channel characteristics, and this procedure can be extended to larger K and N_c values.

In Fig. 11, we consider the first UE and subcarrier $l = 1$ to study the NMSE performance of the dictionaries from the full set of $N_c = 32$ subcarriers and $K = 3$ UEs. For a particular sparsity of $S = 8$, the NMSE value of the CDL-OP dictionary is 1.3×10^{-2} , of the subcarrier K-SVD based dictionary is 1.8×10^{-2} , and of the DFT dictionary is 3.3×10^{-2} . We observe that all the proposed methods' CD have better NMSE performance than the DFT dictionary. Among the proposed methods, the CDL-KSVD method exhibits the poorest NMSE performance. Therefore, we are not pursuing this method any further in the simulations.

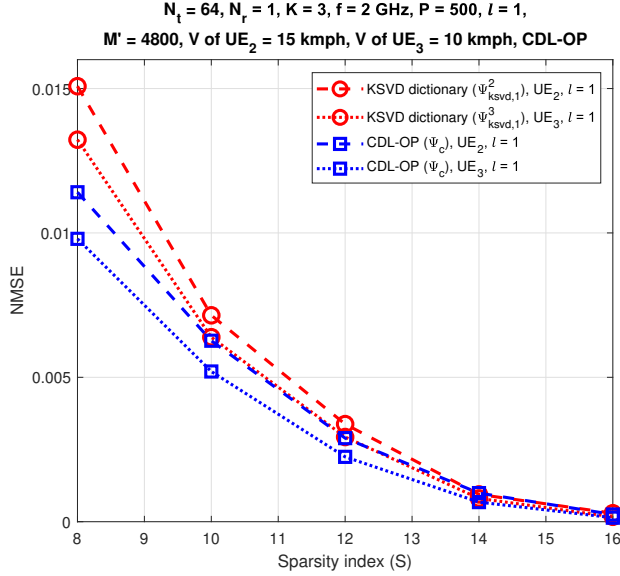


FIGURE 12: In a multi-UE system, the NMSE performance of the K-SVD dictionary and CDL-OP method's dictionary for $K = 3$, $N_t = 64$, $N_r = 1$ and $N_c = 32$. Subcarrier 1 of UE₂ and UE₃ are considered for comparison. Velocities of three UEs are 10, 15, and 20 kmph.

In Fig. 12, the Ψ_c employed for NMSE characterization is learned from the CDL-OP method. Observe from the Fig. 12, for subcarrier $l = 1$ of UE₂ and UE₃ at almost all the sparsity index values, the NMSE values for the proposed CDL-OP method's dictionary is better than subcarrier K-SVD based dictionaries, because the CDL-OP dictionary is learned from the estimated channels of K-SVD based dictionaries.

Experiment 4. In this single-UE experiment, we study the BER performance at the UE as a function of the SNR. The data symbols are transmitted from the BS to the UE in two ways: a) Using the true channel estimates without compression and b) Using the channel estimates with compression that are obtained from the CDL-OP dictionary.

To elaborate further on the performance of our proposed framework, we analyze the BER in a downlink scenario. In Fig. 13 we evaluate the BER using two sets of channels: the true uncompressed channels and the channels estimated using the CDL-OP dictionary on subcarrier 1. The precoder matrices employed at the BS are denoted as $\mathbf{W}^g = \text{diag}(\frac{\mathbf{h}_1^H}{|\mathbf{h}_1|})$ and $\mathbf{W}_{op}^g = \text{diag}(\frac{\hat{\mathbf{h}}_{1,op}^H}{|\hat{\mathbf{h}}_{1,op}|})$, which correspond to the weights obtained from the true channels and to the channels estimated using CDL-OP dictionary, respectively. Let \mathbf{x} represents the modulated symbol vector. Explicitly, in our BER analysis, we harness a half-rate convolutional encoder having the generator sequences of $G = [101, 111]$ and the resultant bits are 16-PSK modulated for generating the symbol vector \mathbf{x} . The received signal in the case of true uncompressed channels at the UE can be represented as $y = \mathbf{h}_1^T \mathbf{W}^g \mathbf{x} + n$, where n is the additive noise. Similarly the

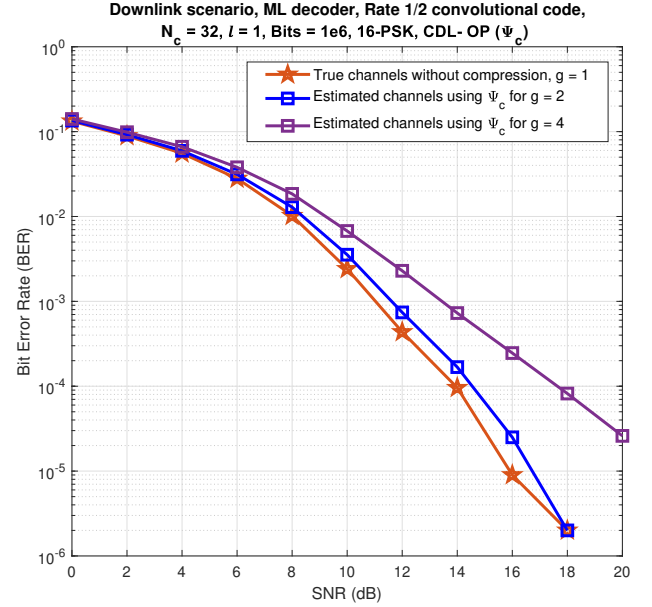


FIGURE 13: In a single-UE system with 64 TAs at the BS and a UE with 1 RA, we examine the BER performance of channel estimates using the CDL-OP methods' dictionary. We consider two scenarios: $N_g = N_r N_t / 2$ and $N_g = N_r N_t / 4$. For comparison, we assume uncompressed channel estimates for subcarrier 1. The UE has a velocity of 20 kmph.

received signal for channels estimated using the CDL-OP dictionary can be represented as $y_{op} = \hat{\mathbf{h}}_1^T \mathbf{W}_{op}^g \mathbf{x} + n$.

The CDL-OP dictionaries used in this experiment are learned at a sparsity of 16 for $g = 2$ and at a sparsity of 8 for $g = 4$. As we increase the compression factor g to reduce the CSI feedback from the UE, we observe a BER performance erosion. The lower bound shown in Fig. 13 represents the BER performance when the BS employs uncompressed CSI. Notably, as depicted in Fig. 13, the BER of the UE, recorded for $g = 2$ when utilizing the CDL-OP dictionary approaches the lower bound.

V. Summary and Conclusions

We proposed a novel CDL framework for reducing the FDCHTF feedback and memory requirement of the UE and BS. The framework is more beneficial for the UE, which is usually resource-constrained, and the savings can be significant. For the simulations, the channels are generated using the QuaDRiGa simulator. In a multi-UE system of three UEs and in a single-UE system, all the proposed method's dictionaries have better NMSE performance than the DFT dictionary. The CDL-OP dictionary performs better than the CDL-KSVD dictionary for all the sparsities. Hence the CDL-OP method can be beneficially employed for CDL to compress the CSI and improve the CSI reconstruction performance. In terms of the computational complexity, the CDL-OP method requires only a single SVD operation to learn the CD, while the CDL-KSVD method requires an

SVD operation for learning each column in the CD. So the CDL-OP method has lower computational complexity than the CDL-KSVD method. To minimize the impact imposed on the BER performance, it is important to choose an appropriate compression ratio g . In our case, a compression ratio of $g = 2$ is considered to have a modest impact on the BER performance. By selecting a suitable compression ratio, the system can strike a balance between reducing the amount of feedback, while maintaining a satisfactory BER performance.

We conclude by highlighting the differences between the multi-UE and single-UE systems as follows:

- 1) In the multi-UE system, the memory is reduced by a factor of N_c at the UE and KN_c at the BS by having only a single CD instead of multiple subcarrier dictionaries. For $N_t = 64$ and $N_c = 32$, the memory required for storing the CD at each UE is reduced by a factor of 32 and the CSI feedback is reduced by a factor of two.
- 2) In the single-UE system, the memory is reduced by a factor of N_c at both the UE and BS, the dictionary feedback is also reduced by a factor of N_c in the uplink. This is achieved by sending only a single CD instead of N_c subcarrier dictionaries to the BS. For $N_t = 64$ and $N_c = 32$, the memory is reduced by a factor of 32 for storing only a CD, and the dictionary feedback is also reduced by a factor of 32. Finally, the CSI feedback is reduced by a factor of two.
- 3) In the multi-UE system, the CD (Ψ_c) generated using the CDL-OP has a better NMSE performance to that of the individual subcarrier K-SVD dictionaries $\Psi_{ksvd,l}^k \forall l \in [1, N_c], \forall k \in [1, K]$.
- 4) In the single-UE system, the CD (Ψ_c) generated using the CDL-OP method has a better NMSE performance to that of the individual subcarrier K-SVD dictionaries $\Psi_{ksvd,l} \forall l \in [1, N_c]$.

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